

A NOVEL METHOD FOR THE DESIGN OF SWITCHING SURFACES FOR DISCRETIZED MIMO NONLINEAR SYSTEMS

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Designing variable structure control with sliding mode (VSC-SM) control schemes needs a switching function or a sliding surface which guarantees the global stability of the closed-loop system. Despite the fact that a wide range of design approaches has been proposed for solving this mathematical problem, the number of proposed methodologies for nonlinear systems is not very extensive, especially for discrete time nonlinear MIMO systems, and most of them require some coordinate system transformation. Therefore, it is not an easy task to find a design scheme that can be applied to discrete time nonlinear MIMO systems. The proposed methodology introduces a mathematical tool: a switching surface equation for a class of MIMO nonlinear systems through an explicit equation without any coordinate transformation. This equation makes use of an implicit linearizing process via the Taylor expansion that allows the use of linear procedures for the design of switching surfaces and the forward Euler method to obtain a discrete time dynamics representation. An illustrative example is included to show the advantages of the proposed design methodology.

Keywords: discrete sliding mode, variable structure control, nonlinear control, optimal control, MIMO systems.

1. Introduction

The procedure for designing VSC-SM consists of two steps. Firstly, designing a switching function or a sliding surface that guarantees the global stability of the closed loop system, and secondly, specifying a control law that assures the existence of a stable sliding mode. The first step is related to the closed-loop sliding phase or steady state controlled system dynamics, and the second one to the reaching phase or transient state system dynamics. Therefore, the performance of the steady state of the controlled system depends on the switching function parameters. The earliest works on VSC-SM covered this problem, mainly for continuous linear systems (Utkin, 1977; Utkin and Yang, 1978; Hung *et al.*, 1993; DeCarlo *et al.*, 1988; Gao and Hung, 1993). In the mid-1980s, some detailed studies on *discrete time variable structure control* (DVSC) appeared and, consequently, an increasing number of research works engaged in analyzing and

specifying discrete time sliding surfaces were carried out (Furuta, 1990; Gao *et al.*, 1995).

For sliding surface design in the context of linear systems, the research lines are based on classical linear system design methods such as arbitrary eigenvalues assignment (Ackermann and Utkin, 1994; Utkin *et al.*, 1999; Perruquetti and Barbot, 2002; Draženović *et al.*, 2013) or optimal control approaches (Tapia *et al.*, 2014; Kim *et al.*, 2000; Choi, 2003; Edwards and Spurgeon, 2003; Lin *et al.*, 2013). On the other hand, for nonlinear systems, a reduced number of results have been reported. Nevertheless, the problem has been analyzed since the mid-1980s (DeCarlo *et al.*, 1988; Sira-Ramírez, 1986; 1991; Spurgeon and Davies, 1993; Su *et al.*, 1996; Ghaffari and Yazdanpanah, 2008; Zhang *et al.*, 2010; Rui and Dong-wei, 2011; Nadzinski *et al.*, 2012).

The most general methodology consists in obtaining a nonlinear canonical dynamics representation (reduced canonical form, normal canonical form, Brunovsky's

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canonical form, etc.), and then the switching surface is calculated in the new state space coordinates. Representations in normal and Brunovsky's canonical forms are most commonly used (Sira-Ramírez, 1991), but cannot be applied to nonminimum phase plants.

On the other hand, if a coordinate transformation is used, then the switching surface specification is made in the new coordinate system, and therefore an inverse transformation is needed in order to obtain knowledge about the dynamics in the original one. Furthermore, for high order plants, the complexity of these approaches increases considerably and finding the solution becomes a difficult task. In addition, existing research works are based on the ideal *sliding mode* (SM) dynamics, i.e., they do not take into consideration the nonideal behaviour of the SM inherent to DVSC (Gao et al., 1995; Sira-Ramírez, 1991; Milosavljević, 1985; Potts and Yu, 1991; Furuta and Pan, 1995). These nonideal dynamics, known as the quasi-sliding or pseudo-sliding mode, consist of undesirable oscillatory vector state trajectories around the switching surface. These drawbacks (the lack of design methodologies, the complexity of the few existent ones and the need for considering quasi-sliding mode dynamics) motivate our research work, whose main objective is to find an easy way for specifying a stable sliding manifold for discrete time nonlinear multi-input-multi-output (MIMO) systems considering the nonideal SM dynamics in the design procedure.

The proposed design methodology is based on a new versatile switching surface equation applied to obtaining an MIMO discrete time nonlinear system with the following main features: (i) the switching surface equation has the same structure regardless of the system nonlinearities dynamics, (ii) the complexity of applying the methodology does not vary with the order of the plant, (iii) some parameters of the proposed equation allow obtaining different steady state performances according to various design criteria such as optimal control methods or eigenvalue assignment approaches, (iv) the proposed methodology does not need any coordinate transformation, and (v) a design parameter is considered for the adjustment of the nonideal sliding mode system dynamics.

All these features make the methodology a useful tool. Indeed, the designer can vary some parameters of the equation to obtain several switching surfaces and, consequently, a comparison of the resultant sliding mode dynamics with other techniques can be made.

Finally, it is important to stress that, for achieving the switching surface scheme, the forward Euler time stepping method (or the explicit Euler method) is used to obtain a discrete time difference equation approximation and the Taylor expansion is applied to linearize the system. In the work is introduced of Draženović et al. (2013), a decoupled solution for designing switching

surfaces applied to linear continuous and discrete time systems without any transformation using a state feedback gain matrix which can be chosen using eigenvalues or optimal methodologies. The main advantage of the proposed methodology, compared with this approach, is that it includes a design parameter which allows the adjustment of the sliding mode dynamics of the controlled system.

An overview of the general sliding hyperplane designing problem related to MIMO nonlinear systems is presented in Section 2. The remainder of the paper is organized as follows: the proposed design method is developed in Section 3, an illustrative design example is detailed in Section 4, and conclusions and future proposals are presented in Section 5.

Throughout this paper, the following notation is used: $f : \mathbb{R}^m \rightarrow \mathbb{R}^n$ stands for a function that maps from the m -dimensional vector space \mathbb{R}^m to the n -dimensional vector space \mathbb{R}^n ; $\|\cdot\|$ denotes the magnitude of a scalar or the standard *Euclidean* norm of a vector; $|\cdot|$ indicates the absolute value of a scalar; $\text{sign}(\cdot)$ stands for the sign of a real scalar and $\det(\cdot)$ for the determinant of a square matrix; I_m means the $m \times m$ identity matrix; $\mathcal{N}(\cdot)$ represents the null space of a matrix; $\mathcal{R}(\cdot)$ denotes the range of a matrix and $\Lambda(\cdot)$ means the set of eigenvalues of a square matrix. Finally, $\mathcal{P}(\cdot)$ denotes a generic system or process.

2. Preliminaries

VSC and DVSC are control schemes where the input laws $\mathbf{u} : \mathbb{R}^m \rightarrow \mathbb{R}^n$ are generally noncontinuous functions that depend on the value of some switching function $s : \mathbb{R}^n \rightarrow \mathbb{R}^m$ such that the state of the systems, denoted as $\mathbf{x} \in \mathbf{X} \subset \mathbb{R}^n$, is steered from some initial state $\mathbf{x}(0) \in \mathbf{X}$ to a subspace region $\mathcal{S} = \{\mathbf{x} \in \mathbf{X} : s(\mathbf{x}) = 0\}$. Therefore, the system state remains indefinitely on \mathcal{S} , i.e., the state *slides* on the surface. Consequently, \mathcal{S} is known as a switching surface and, once the state arrives and lies on the switching surface, the system is said to be in SM.

A particular feature of VSC (see Fig. 1) is that these controllers are built with two main parts: the first one is a multivariable function known as a switching surface (the box labelled as $s(\mathbf{x}(k))$ in the figure) and a bank of control law blocks or a big multivariable function that makes use of the output of the switching surface in order to obtain the desired control action $\mathbf{u}(k)$ to the plant. As previously mentioned, the aim of this work is to give a new methodology for the design switching surfaces applied to MIMO nonlinear systems. The general nonlinear sliding surface problem can be stated as follows.

Problem 1. Consider a nonlinear discrete time system

whose dynamics are defined as

$$\begin{aligned} \mathbf{x}(k+1) &= \mathbf{f}(\mathbf{x}(k), \mathbf{u}(k), k), \\ \mathbf{y}(k) &= \mathbf{h}(\mathbf{x}(k), \mathbf{u}(k), k), \end{aligned} \quad (1)$$

where $\mathbf{x} \in \mathbf{X} \subset \mathbb{R}^n$, $\mathbf{u} \in \mathbf{U} \subset \mathbb{R}^m$ and $\mathbf{y} \in \mathbf{Y} \subset \mathbb{R}^p$ are the state, input and output vectors, respectively, and $f : \mathbf{X} \times \mathbf{U} \rightarrow \mathbf{X}$ and $h : \mathbf{X} \times \mathbf{U} \rightarrow \mathbf{Y}$ are supposed to be analytical functions. Then, given a control law $u(k)$ such that a sliding mode on the surface \mathcal{S} is ensured:

$$\mathcal{S} = \{\mathbf{x} \in \mathbf{X} \mid \mathbf{s}(\mathbf{x}(k)) = 0\}, \quad (2)$$

the switching function $\mathbf{s} : \mathbf{X} \rightarrow \mathbb{R}^m$ must be specified to make the closed-loop system asymptotically stable.

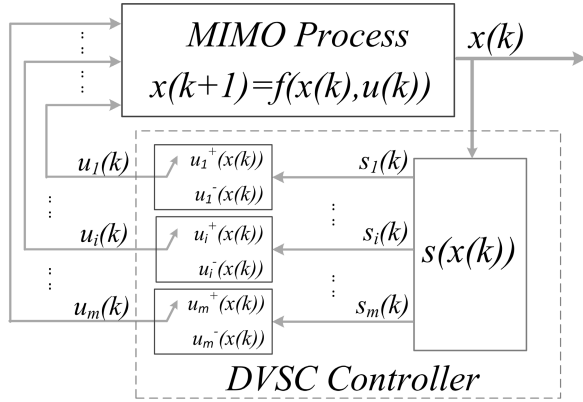


Fig. 1. General DVSC scheme.

It has been mentioned that the number of research works related to the design of switching surfaces applied to nonlinear systems is considerably smaller than for linear ones. One of the earliest works related to nonlinear sliding surface design was presented by Sira-Ramírez (1986), who proposed to obtain a linearized equivalent representation via state feedback, where a linear sliding surface is designed in Brunovsky's canonical form. Other approaches make use of linear approximations as in the work of Camacho and Smith (2000), where nonlinear systems are approximately modelled via *first order plus dead time* (FOPDT). In another work, Sira-Ramírez (1991) proposed the use of the normal canonical representation for the design of DVSC for nonlinear systems, but without any indication or guideline about how the switching sliding surfaces are chosen. DeCarlo *et al.* (1988) presented a method for designing SM surfaces using regular canonical representations (Johansson and Nunes, 1998), and Spurgeon and Davies (1993) made use of a noncanonical transformation. Su *et al.* (1996; 1994) set forth a *Lyapunov* approach for sliding surface design. More recently, Ghaffari and Yazdanpanah (2008) proposed a method for computing nonlinear stable sliding mode surfaces, and Rui and Dong-wei (2011)

introduced an algorithm for designing optimal sliding surface for nonlinear discrete time systems using the nonlinear *two point boundary problem* (TPBV) approach, while Bartoszewicz and Leśniewski (2014) made use of an optimal approach for designing a sliding hyperplane. Finally, some approaches intended to apply DVSC with an SM to discrete time nonlinear systems based on *T-S fuzzy models* use linear methods such as LMI for the design of switching surfaces (Zhang *et al.*, 2010; Nadzinski *et al.*, 2012).

Before presenting the design of sliding surfaces applied to nonlinear systems, let us find the ideal SM dynamics. Consider a nonlinear discrete time system whose dynamics are defined in (1). Then the equivalent control law $u_{equ}(k)$ can be found so that

$$\mathbf{s}(k+1) = \mathbf{s}(k) = 0, \quad (3)$$

where

$$\mathbf{s}(k+1) = \mathbf{s}(\mathbf{f}(\mathbf{x}(k), \mathbf{u}_{equ}(k), k)). \quad (4)$$

This equation yields the ideal sliding mode described as

$$\begin{aligned} \mathbf{x}(k+1) &= \mathbf{f}(\mathbf{x}(k), \mathbf{u}_{equ}(k), k), \quad k \in \mathbb{Z}^+, \\ \mathbf{s}(\mathbf{x}(k)) &= 0, \quad \forall k. \end{aligned} \quad (5)$$

For a linear switching surface $\mathbf{s}(k) = \mathbf{C}\mathbf{x}(k)$ and from (1), we obtain

$$\mathbf{C}\mathbf{f}(\mathbf{x}(k), \mathbf{u}_{equ}(k), k) = 0. \quad (6)$$

Therefore

$$\mathbf{u}_{equ}(k) = \mathbf{f}^{-1}(\mathbf{x}(k), \mathbf{u}(k), k), \quad (7)$$

which implies that \mathbf{u}_{equ} can be unequivocally found if \mathbf{f} is single-valued or regular.

In the case of affine systems, i.e., those whose dynamics exhibit a linear behaviour in relation to the inputs and a nonlinear one with respect to the states, (1) can be written as

$$\mathbf{x}(k+1) = \mathbf{f}(\mathbf{x}(k), k) + \mathbf{\Gamma}\mathbf{u}(k), \quad (8)$$

where $\mathbf{\Gamma} : \mathbf{X} \rightarrow \mathbf{X} \times \mathbf{U}$. Thus, the ideal sliding surface dynamic are defined as

$$\mathbf{s}(k) = \mathbf{C}\mathbf{f}(\mathbf{x}(k), k) + \mathbf{C}\mathbf{\Gamma}\mathbf{u}(k), \quad (9)$$

and the equivalent control law is given by

$$\mathbf{u}_{equ}(k) = -(\mathbf{C}\mathbf{\Gamma})^{-1} \mathbf{C}\mathbf{f}(\mathbf{x}(k), k). \quad (10)$$

Therefore, the closed loop ideal SM is described as

$$\mathbf{x}(k+1) = [\mathbf{I}_n - \mathbf{\Gamma}(\mathbf{C}\mathbf{\Gamma})^{-1}\mathbf{C}]\mathbf{f}(\mathbf{x}(k), k). \quad (11)$$

In general, the methods for designing nonlinear surfaces are based on obtaining a suitable canonical representation in order to find an easy mathematical model that could help in the design process (Hung *et al.*, 1993; DeCarlo *et al.*, 1988; Gao and Hung, 1993; Sira-Ramírez 1986; 1991; Spurgeon and Davies, 1993; Su *et al.*, 1994). The following section presents a new scheme for designing sliding switching surfaces applied to MIMO discrete time nonlinear systems, which simplifies the design tasks and gives a high level of accuracy for an arbitrary location of eigenvalues or optimal SM dynamics, depending on the desirable design criteria.

3. Proposed sliding hyperplane design: The main results

A novel sliding surface equation is introduced in the next theorem.

Theorem 1. *Suppose that we are given the following:*

1. a MIMO nonlinear continuous time system $\mathcal{P}(\cdot)$ with dynamics described as

$$\dot{\mathbf{x}}(t) = \mathbf{f}(\mathbf{x}(t), \mathbf{u}(t)), \quad (12)$$

where $\mathbf{x} \in \mathbf{X} \subset \mathbb{R}^n$ is the state vector and $\mathbf{f} : \mathbb{R}^{n+m} \rightarrow \mathbb{R}^n$ defined as

$$\mathbf{f}(x) = \begin{bmatrix} f_1(x, u) & f_2(x, u) & \cdots & f_n(x, u) \end{bmatrix}^T, \quad (13)$$

where every $f_i : \mathbb{R}^{n+m} \rightarrow \mathbb{R}$ is a smooth nonlinear function;

2. a state feedback gain matrix $\mathbf{K} \in \mathbb{R}^{m \times n}$ such that the following system dynamics are asymptotically stable:

$$\mathbf{x}(k+1) = [\hat{\mathbf{\Phi}} - \hat{\mathbf{\Gamma}}\mathbf{K}]\mathbf{x}(k), \quad (14)$$

where $\hat{\mathbf{\Phi}}$ and $\hat{\mathbf{\Gamma}}$ are defined as

$$\begin{aligned} \hat{\mathbf{\Phi}} &= \mathbf{I}_n + T\mathbf{J}_A, \\ \hat{\mathbf{\Gamma}} &= T\mathbf{J}_B, \end{aligned} \quad (15)$$

\mathbf{I}_n being the n -th order identity matrix, T sample time and \mathbf{J}_A and \mathbf{J}_B the Jacobian matrix of $\mathbf{f}(x)$ with respect to $\mathbf{x}(t)$ and $\mathbf{u}(t)$, respectively, such that

$$\begin{aligned} \mathbf{J}_A(x) &= \left. \frac{\partial \mathbf{f}}{\partial \mathbf{x}} \right|_{x=x_e, u=u_e}, \\ \mathbf{J}_B(x) &= \left. \frac{\partial \mathbf{f}}{\partial \mathbf{u}} \right|_{x=x_e, u=u_e}, \end{aligned}$$

where $\mathbf{x}_e \in \mathbf{X}$ is an equilibrium state.

If $\mathcal{P}(\cdot)$ is controlled via DVSC, then the switching function $\mathbf{s}(k) = \mathbf{C}\mathbf{x}(k)$ makes the discrete time ideal sliding mode of the controlled system asymptotically stable around $\mathbf{x}_e \in \mathbf{X}$ if \mathbf{C} is estimated as

$$\mathbf{C} = \mathbf{E}\mathbf{K}[\mathbf{I}_n + T\mathbf{J}_A(x)]^{-1}, \quad (16)$$

where $\mathbf{E} \in \mathbb{R}^{m \times m}$ is an arbitrary nonsingular design matrix.

Proof. Let us obtain a linearized system through the first-order term of the Taylor expansion of $\mathbf{f}(\mathbf{x}(t))$ around an equilibrium point \mathbf{x}_e (see Section A.1 in Appendix), i.e., the system dynamics given in (12) are approximated around an equilibrium state \mathbf{x}_e as follows:

$$\dot{\mathbf{x}}(t) \approx \mathbf{A}\mathbf{x}(t) + \mathbf{B}\mathbf{u}(t), \quad (17)$$

where

$$\begin{aligned} \mathbf{A} &= \mathbf{J}_A(x) = \left. \frac{\partial \mathbf{f}}{\partial \mathbf{x}} \right|_{x=x_e, u=u_e}, \\ \mathbf{B} &= \mathbf{J}_B(x) = \left. \frac{\partial \mathbf{f}}{\partial \mathbf{u}} \right|_{x=x_e, u=u_e}. \end{aligned} \quad (18)$$

Then, for time discretization, let us use the Euler method (see Section A.2 in Appendix). Hence, a discrete time system dynamics representation of (17) is equal to

$$\begin{aligned} \mathbf{x}(k+1) &= [\mathbf{I}_n + T\mathbf{A}]\mathbf{x}(k) + T\mathbf{B}\mathbf{u}(k) \\ &= \hat{\mathbf{\Phi}}\mathbf{x}(k) + \hat{\mathbf{\Gamma}}\mathbf{u}(k). \end{aligned} \quad (19)$$

Owing to the condition stated in (14) for the next Lyapunov function, we have

$$V(k) = \mathbf{x}^T(k)\mathbf{P}\mathbf{x}(k), \quad (20)$$

and the following linear Lyapunov equation holds:

$$[\hat{\mathbf{\Phi}} - \hat{\mathbf{\Gamma}}\mathbf{K}]^T \mathbf{P} [\hat{\mathbf{\Phi}} - \hat{\mathbf{\Gamma}}\mathbf{K}] - \mathbf{P} = -\mathbf{Q}, \quad (21)$$

$\mathbf{P} \in \mathbb{R}^{n \times n}$ being a symmetric positive definite matrix and $\mathbf{Q} \in \mathbb{R}^{n \times n}$ a symmetric positive semi-definite matrix.

On the other hand, from (11), and on account of the switching surface $\mathbf{s}(k) = \mathbf{C}\mathbf{x}(k)$, the ideal SM of the system given in (19) is as follows:

$$\begin{aligned} \mathbf{x}_{SM}(k+1) &= [\hat{\mathbf{\Phi}} - \hat{\mathbf{\Gamma}}(\mathbf{C}\hat{\mathbf{\Gamma}})^{-1}\mathbf{C}\hat{\mathbf{\Phi}}]\mathbf{x}(k) \\ &= \hat{\mathbf{\Phi}}_{equ}\mathbf{x}(k). \end{aligned} \quad (22)$$

Taking account of the SM dynamics specified in (22) and applying the Lyapunov theorem to SM stability analysis, the following condition must hold:

$$[\hat{\mathbf{\Phi}} - \hat{\mathbf{\Gamma}}(\mathbf{C}\hat{\mathbf{\Gamma}})^{-1}\mathbf{C}\hat{\mathbf{\Phi}}]^T \mathbf{P} [\hat{\mathbf{\Phi}} - \hat{\mathbf{\Gamma}}(\mathbf{C}\hat{\mathbf{\Gamma}})^{-1}\mathbf{C}\hat{\mathbf{\Phi}}] - \mathbf{P} = -\mathbf{Q}. \quad (23)$$

Since $\mathbf{C} = \mathbf{E}\mathbf{K}\hat{\Phi}^{-1}$, we get

$$\begin{aligned} & [\hat{\Phi} - \hat{\Gamma}(\mathbf{C}\hat{\Gamma})^{-1}\mathbf{E}\mathbf{K}]^T \mathbf{P} [\hat{\Phi} - \hat{\Gamma}(\mathbf{C}\hat{\Gamma})^{-1}\mathbf{E}\mathbf{K}] \\ & \quad - \mathbf{P} = -\mathbf{Q}. \end{aligned} \quad (24)$$

Then, defining $\mathbf{E} = \mathbf{C}\hat{\Gamma}$ without any loss of generality and substituting it into (24), we obtain

$$[\hat{\Phi} - \hat{\Gamma}\mathbf{K}]^T \mathbf{P} [\hat{\Phi} - \hat{\Gamma}\mathbf{K}] - \mathbf{P} = -\mathbf{Q}, \quad (25)$$

which is the same equation as the one given in (21), and this completes the proof. ■

Theorem 1 shows that the sliding surface $\mathbf{s}(k) = \mathbf{C}\mathbf{x}(k)$, where $\mathbf{C} \in \mathbb{R}^{m \times n}$ is defined in (16), guarantees the asymptotic stability of any MIMO nonlinear system represented as in (12) and where a state feedback gain matrix \mathbf{K} is needed. Hence, the problem of designing the sliding surface $\mathbf{s}(k) = \mathbf{C}\mathbf{x}(k)$ is reduced to the specification of the matrix \mathbf{C} so that the characteristic polynomial of $\hat{\Phi}_{CL} = \hat{\Phi} - \hat{\Gamma}\mathbf{K}$ is strictly *Schur* (Åström and Wittenmark, 1997). Additionally, the gain matrix \mathbf{K} can be either estimated via arbitrary eigenvalues assignment approaches or with optimal methods such as the *linear quadratic regulator* (LQR) or the *linear quadratic Gaussian* (LQG). This can be considered an advantage of the proposed methodology because designers can obtain several \mathbf{K} s, and then the evaluation of SM performance can be obtained for every \mathbf{K} . For the pole placement methodology, it is worth mentioning that m eigenvalues of $\hat{\Phi}_{CL}$ must be set to zero, because the equivalent SM always has m poles at the origin (Spurgeon and Pugh, 1991). The other $n - m$ eigenvalues must be set inside the unit circle.

Theorem 2. *If the gain matrix $\mathbf{K} \in \mathbb{R}^{m \times n}$ stabilizes the system via eigenvalue shifting such that the roots of the characteristic polynomial of the matrix*

$$X_{CL}(\lambda) = \det[\lambda\mathbf{I}_n - \hat{\Phi} + \hat{\Gamma}\mathbf{K}] = 0 \quad (26)$$

are located at the arbitrary eigenvalues

$$\lambda_d = \left\{ \lambda_1, \lambda_2, \dots, \lambda_{n-m}, \underbrace{0, 0, \dots, 0}_m \right\}, \quad (27)$$

where $|\lambda_i| < 1, i = 1, 2, \dots, n - m$, then the surface definition $\mathbf{s}(k) = \mathbf{C}\mathbf{x}(k)$ makes the ideal sliding mode of the controlled system asymptotically stable with eigenvalues located exactly at λ_d provided that \mathbf{C} is obtained using (16).

Proof. From the theorem statement, the feedback gain matrix \mathbf{K} stabilizes the system, where the closed-loop system dynamics are given by

$$\mathbf{x}_{CL}(k+1) = [\hat{\Phi} - \hat{\Gamma}\mathbf{K}]\mathbf{x}(k).$$

If the system is transformed to the canonical form via a similar transformation $\bar{\mathbf{x}}(k) = \mathbf{M}\mathbf{x}(k)$, then the dynamics of the closed-loop canonical system are given by

$$\bar{\mathbf{x}}_{CL}(k+1) = [\bar{\Phi} - \bar{\Gamma}\bar{\mathbf{K}}]\bar{\mathbf{x}}(k), \quad (28)$$

where $\bar{\Phi} = \mathbf{M}\hat{\Phi}\mathbf{M}^{-1}$, $\bar{\Gamma} = \mathbf{M}\hat{\Gamma}$ and $\bar{\mathbf{K}} = \mathbf{K}\mathbf{M}^{-1}$ and \mathbf{M} is given as

$$\mathbf{M} = \begin{bmatrix} \mathbf{g}_{m_1} \\ \mathbf{g}_{m_1}\hat{\Phi} \\ \vdots \\ \mathbf{g}_{m_1}\hat{\Phi}^{m_1-1} \\ \mathbf{g}_{m_1+m_2} \\ \mathbf{g}_{m_1+m_2}\hat{\Phi} \\ \vdots \\ \mathbf{g}_{m_1+m_2}\hat{\Phi}^{m_2-1} \\ \vdots \\ \mathbf{g}_{m_1+\dots+m_p} \\ \mathbf{g}_{m_1+\dots+m_p}\hat{\Phi}^{m_p-1} \end{bmatrix}, \quad (29)$$

with \mathbf{g}_i is being the i -th row of the rearranged controllability matrix $\bar{\mathbf{W}}_c$ obtained from \mathbf{W}_c as follows:

$$\begin{aligned} \bar{\mathbf{W}}_c(\bar{\Phi}, \bar{\Gamma}) = & \begin{bmatrix} \bar{\Gamma}_1 & \bar{\Phi}\bar{\Gamma}_1 & \dots & \bar{\Phi}^{m_1-1}\bar{\Gamma}_1; \\ \bar{\Gamma}_2 & \bar{\Phi}\bar{\Gamma}_2 & \bar{\Phi}^{m_2-1}\bar{\Gamma}_2 \\ \dots & \dots & \dots & \dots \\ \bar{\Gamma}_{m_i} & \bar{\Phi}\bar{\Gamma}_{m_i} & \dots & \bar{\Phi}^{m_p-1}\bar{\Gamma}_{m_i} \end{bmatrix}, \end{aligned} \quad (30)$$

where $\sum_{i=1}^p m_i = n$. It is known that a similar transformation is invariant to the eigenvalue location, and therefore the eigenvalues of $[\bar{\Phi} - \bar{\Gamma}\bar{\mathbf{K}}]$ are λ_d . As for the ideal SM of the system in the canonical form, we have

$$\bar{\mathbf{x}}_{SM}(k+1) = [\bar{\Phi} - \bar{\Gamma}(\bar{\mathbf{C}}\bar{\Gamma})^{-1}\bar{\mathbf{C}}\bar{\Phi}]\hat{\mathbf{x}}(k). \quad (31)$$

Comparing (28) and (22), it is clear that if the following condition is fulfilled:

$$\bar{\mathbf{K}} = (\bar{\mathbf{C}}\bar{\Gamma})^{-1}\bar{\mathbf{C}}\bar{\Phi}, \quad (32)$$

then the eigenvalues of the ideal SM matrix are located at λ_d . Also, let us consider the following representation for $\bar{\mathbf{C}}$ and $\bar{\Gamma}$:

$$\begin{aligned} \bar{\mathbf{C}} = & [\bar{\mathbf{c}}_1 \quad \bar{\mathbf{c}}_2 \quad \dots \quad \bar{\mathbf{c}}_n], \quad (33) \\ \bar{\Gamma} = & \begin{bmatrix} \mathbf{0}_{m_1-1 \times m} \\ \mathbf{F}_1 \\ \mathbf{0}_{m_2-1 \times 1} \\ \mathbf{F}_2 \\ \vdots \\ 0 \\ \mathbf{F}_m \end{bmatrix}, \end{aligned}$$

where $\bar{c}_i \in \mathbb{R}^m$ is the i -th column of $\mathbf{C} \in \mathbb{R}^m$. Defining the matrix $\mathbf{F} \in \mathbb{R}^{m \times m}$ as

$$\mathbf{F} = \begin{bmatrix} \mathbf{F}_1 \\ \mathbf{F}_2 \\ \vdots \\ \mathbf{F}_m \end{bmatrix} \quad (34)$$

and taking account of the fact that

$$\mathbf{F}_i = [0 \ 0 \ \cdots \ 1 \ * \ \cdots \ *]$$

we conclude that \mathbf{F} is an upper triangular matrix in which all the elements on the main diagonal are ones. Therefore, $\det(\mathbf{F}) = 1$. In addition, it can be shown that

$$\bar{\mathbf{C}}\bar{\mathbf{\Gamma}}\mathbf{F}^{-1} = \mathbf{L} \quad (35)$$

$$= [c_{m_1} \ c_{m_1+m_2} \ \cdots \ c_n]. \quad (36)$$

Thus, if \mathbf{L} is arbitrarily specified such that $\det(\mathbf{L}) = \alpha$, $\alpha \neq 0$, since $\det(\mathbf{F}^{-1}) = 1$, we get $\det(\bar{\mathbf{C}}\bar{\mathbf{\Gamma}}) = \alpha \neq 0$. Defining $\mathbf{E} = \mathbf{F}\mathbf{L}\mathbf{F} = \bar{\mathbf{C}}\bar{\mathbf{\Gamma}}$ and replacing $\bar{\mathbf{C}}\bar{\mathbf{\Gamma}}$ into (32), we obtain

$$\bar{\mathbf{K}} = \mathbf{E}^{-1}\bar{\mathbf{C}}\bar{\mathbf{\Phi}}. \quad (37)$$

Therefore

$$\bar{\mathbf{C}} = \mathbf{E}\bar{\mathbf{K}}\bar{\mathbf{\Phi}}^{-1}. \quad (38)$$

Finally, from $\mathbf{C} = \bar{\mathbf{C}}\mathbf{M}$, $\bar{\mathbf{K}} = \mathbf{K}\mathbf{M}^{-1}$ and $\mathbf{M}^{-1}\bar{\mathbf{\Phi}}^{-1}\mathbf{M} = \hat{\mathbf{\Phi}}^{-1}$, it follows that

$$\mathbf{C} = \mathbf{E}\mathbf{K}\hat{\mathbf{\Phi}}^{-1}. \quad (39)$$

■

Corollary 1. Under the assumptions of Theorem 2, we have $\mathbf{E} = \mathbf{C}\hat{\mathbf{\Gamma}}$ when \mathbf{K} fulfills (26) and (27).

From Theorem 2, the spectrum of the ideal SM dynamics, denoted as $\Lambda(\hat{\mathbf{\Phi}}_{equ})$, have m zero eigenvalues and the same $n - m$ eigenvalues chosen for the stable dynamics of $\hat{\mathbf{\Phi}}_{CL}$, i.e., $\Lambda(\hat{\mathbf{\Phi}}_{CL}) = \Lambda(\hat{\mathbf{\Phi}}_{equ})$, where $\hat{\mathbf{\Phi}}_{equ}$ is given in (22). As shown in Theorem 2, the sliding surface definition (16) presents a simple way to configure the SM dynamics by means of an arbitrary eigenvalues assignment and it is easy to check that the eigenvalues of the resultant ideal SM system matrix are located exactly at the desired eigenvalues. What is more, the theorem can be proven easier, with the hint chosen intended to prove that the ideal sliding mode is completely specified by \mathbf{K} . Moreover, if the arbitrary matrix \mathbf{E} is chosen such that $\mathbf{E} = \mathbf{C}\hat{\mathbf{\Gamma}} \neq 0$, then the SM invariance property is guaranteed (Dorling and Zinober, 1986). Since $\mathbf{C}\hat{\mathbf{\Gamma}} \neq 0$, we have $\mathcal{R}(\mathbf{\Gamma}) \cap \mathcal{N}(\mathbf{C}) = \emptyset$, which implies that \mathbf{E} does not affect the ideal SM dynamics and, therefore, they are exclusively specified by the gain matrix \mathbf{K} .

However, Milosavljević (1985) proved that for discrete time systems the ideal SM cannot be achieved

and a quasi-or pseudo-sliding mode appears. In the quasi-sliding mode, the state vector oscillates in a region around $\mathbf{s}(k) = 0$ and control laws are designed for minimizing the amplitude of oscillations. Hence, calculating the nonideal SM dynamics yields

$$\mathbf{s}(k+1) = \mathbf{E}[\mathbf{K}\mathbf{x}(k) + \mathbf{u}(k)]. \quad (40)$$

Then it is obvious that $\mathbf{s}(k+1)$ depends on \mathbf{E} . Indeed, every $\mathbf{s}_i \in \mathbf{s}(k)$ can be adjusted through a linear combination of the components of the vector $\mathbf{u}(k)$. Consequently, \mathbf{E} should be considered when the control laws are specified. It is important to note that if the state feedback gain matrix \mathbf{K} does not fulfill the conditions given in (26) and (27), then $\mathbf{E} \neq \mathbf{C}^{-1}\hat{\mathbf{\Gamma}}$. However, it can be shown that a desired $\mathbf{C}\hat{\mathbf{\Gamma}} = \mathbf{D}$ can be achieved if \mathbf{E} is defined as follows:

$$\mathbf{E} = \mathbf{D}(\mathbf{K}\hat{\mathbf{\Phi}}^{-1}\hat{\mathbf{\Gamma}})^{-1}. \quad (41)$$

In addition, some relevant features that are very helpful during the design of control laws are given in the following lemma.

Lemma 1. Consider $\mathcal{P}(\mathbf{x}, \mathbf{u})$, a linearized and discretized MIMO system whose dynamics are described by (19). If $\mathcal{P}(\mathbf{x}, \mathbf{u})$ is controlled using a DVSC and the switching surface is defined as in (16) such that the restrictions (26) and (27) are fulfilled, then the ideal SM equivalent control $\mathbf{u}_{equ}(k)$ is equal to

$$\mathbf{u}_{equ}(k) = -\mathbf{K}\mathbf{x}(k), \quad (42)$$

and the ideal SM dynamics are

$$\mathbf{s}(k+1) = \mathbf{s}(k) = 0, \quad (43)$$

$$\mathbf{x}_{equ}(k+1) = \hat{\mathbf{\Phi}}_{equ}\mathbf{x}(k), \quad (44)$$

where

$$\hat{\mathbf{\Phi}}_{equ} = \hat{\mathbf{\Phi}} - \mathbf{\Gamma}\mathbf{K}. \quad (45)$$

Proof. Note that the proof is immediate if we set $\mathbf{C} = \mathbf{E}\mathbf{K}\hat{\mathbf{\Phi}}^{-1}$ in (10) and (11). ■

This lemma introduces two important features: (i) the equivalent control law is similar to the classical state feedback control law for pole placement, and (ii) the equivalent system dynamics do not depend on \mathbf{e} and are exactly the same as for the system controlled using and state space feedback scheme.

Considering Theorem 1, the proposed design method can be described as follows:

1. Obtain the matrices $\hat{\mathbf{\Phi}}$ and $\hat{\mathbf{\Gamma}}$ using (15) and (18). The sampling time T can be obtained from the system step response using the Åström criterion (Åström and Wittenmark, 1997), which establishes that the sampled time T can be calculated from the system

step response so that, during the rise time t_r , the number of samples N_r must be between 4 and 10, i.e.,

$$N_r = \frac{t_r}{T} = 4 \sim 10. \quad (46)$$

2. Find the gain matrix \mathbf{K} so that $\hat{\Phi}_{CL} = \hat{\Phi} - \hat{\Gamma}\mathbf{K}$ is strictly Schur.
3. Find any desired $\mathbf{C}\Gamma$ according to the desired performance of the *pseudo-sliding* system dynamics. If \mathbf{K} is found using eigenvalue placement, then $\mathbf{E} = \mathbf{C}\Gamma$, otherwise use the equation given in (41). If no specific $\mathbf{C}\Gamma$ definition is given, choose an arbitrary matrix \mathbf{E} .
4. Compute \mathbf{C} using (16).
5. Verify that the characteristic polynomial of $\hat{\Phi}_{equ}$ is strictly Schur.

Once the switching surface is completely defined, a control law $u(k)$ which fulfills some reaching law restriction such as the ones given by Gao *et al.* (1995), Sira-Ramírez (1991), Bartoszewicz (1998) or Furuta and Pan (2002) is needed. In addition, the design procedure explained so far considers plants without uncertainties about their dynamics. It is known (Gao *et al.*, 1995) that perturbed systems controlled via DVSC whose dynamics are given as follows:

$$\begin{aligned} \mathbf{x}(k+1) &= (\tilde{\Phi} + \Delta\tilde{\Phi})\mathbf{x}(k) \\ &\quad + \hat{\Gamma}u(k) + \mathbf{d}(k) \end{aligned} \quad (47)$$

are invariant with respect to system deviations $\Delta\tilde{\Phi}$ and external perturbations $\mathbf{d}(k)$ when the following matching conditions hold:

$$\begin{aligned} \Delta\tilde{\Phi} &= \hat{\Gamma}\tilde{\Phi}, & \tilde{\Phi} &\in \mathbb{R}^{m \times n}, \\ \mathbf{d}(k) &= \hat{\Gamma}\tilde{\mathbf{d}}(k), & \tilde{\mathbf{d}} &: \mathbb{R} \rightarrow \mathbb{R}^m, \end{aligned} \quad (48)$$

and $\det(\mathbf{E}) \neq 0$.

However, the control law $\mathbf{u}(k)$ must be designed such that some reaching law must be fulfilled considering these uncertainties, mostly when the matching conditions are not achieved (Furuta, 1990; Gao *et al.*, 1995; Kim *et al.*, 2000; Sira-Ramírez, 1991; Yu *et al.*, 2000; Yadav and Singh, 2012; Mondal *et al.*, 2012; Qu *et al.*, 2014). This part of the design of DVSC controllers is not directly carried out during switching the surface design phase. Additional design problems, such as unobservable states, can be minimized using state vector estimation or predictors (see, e.g., Pai, 2008; Wang *et al.*, 2011). In addition, it is known that for discrete time systems (Soroush and Kravaris, 1992) delays only modify the relative degree of the state space dynamics. Thus, time delay compensation can be made using some additional scheme such as the one proposed by Sira-Ramírez (1991).

4. Example

An industrial process used as a MIMO example is applied. It includes level control of a four-tank laboratory system (Gatzke *et al.*, 2000). This nonlinear system consists of four-tanks T_1, T_2, T_3 and T_4 with the cross-sectional area A_i , $i = 1, \dots, 4$, respectively, and where two pumps (system inputs) are used for transferring water from a bottom basin into four upper tanks (see Fig. 2). The output flow rate for each pump $u_1(t)$ and $u_2(t)$ can be manipulated to control the two level outputs $h_1(t)$ and $h_2(t)$, respectively. The system exhibits interacting multivariable dynamics because it was designed such that $u_1(t)$ and $u_2(t)$ affect $h_1(t)$ and $h_2(t)$. The continuous time system model dynamics are as follows:

$$\begin{aligned} \dot{h}_1(t) &= -\frac{1}{A_1} \left[a_1 \sqrt{2gh_1(t)} - a_3 \sqrt{2gh_3(t)} \right] \\ &\quad + \frac{1}{A_1} \gamma_1 k_1 u_1(t), \\ \dot{h}_2(t) &= -\frac{1}{A_2} \left[a_2 \sqrt{2gh_2(t)} - a_4 \sqrt{2gh_4(t)} \right] \\ &\quad + \frac{1}{A_2} \gamma_2 k_2 u_2(t), \\ \dot{h}_3(t) &= -\frac{1}{A_3} \left[a_3 \sqrt{2gh_3(t)} - (1 - \gamma_2) k_2 u_2(t) \right], \\ \dot{h}_4(t) &= -\frac{1}{A_4} \left[a_4 \sqrt{2gh_4(t)} - (1 - \gamma_1) k_1 u_1(t) \right], \\ y(t) &= \begin{bmatrix} 1 & 1 & 0 & 0 \end{bmatrix} h(t), \end{aligned} \quad (49)$$

where $d_1(t)$ and $d_2(t)$ are the deviation and perturbation signals, $g \simeq 980 \text{ cm/s}^2$ is the gravitational acceleration, a_i and A_i correspond to the drain and the tank area of the i -th tank, respectively, and where γ_1 and γ_2 denote the ratio flow in Tank 1 and Tank 4 and the ratio flow in Tank 2 to Tank 3, respectively, such that $\gamma_1 + \gamma_2 < 1$.

The process parameters considered here are $A_i = A = 730 \text{ cm}^2$, $a_1 = a_3 = a_2 = a_4 = 2.3 \text{ cm}^2$, $k_1 = 5.51$, $k_2 = 6.58 \text{ cm}^3/\text{s}$, $u_i^0 = 60\%$, $\gamma_1 = 0.333$ and $\gamma_2 = 0.307$. It is easy to show that, for the inputs $u_1(k) = u_2(k) = 60\%$, the initial state $\mathbf{x}(0) = [14.192 \ 11.243 \ 7.212 \ 4.680]^T$ is a stationary one. Following the proposed methodology, the first step consists in finding the Jacobian matrices $\mathbf{J}_A, \mathbf{J}_B$. Hence

$$\mathbf{J}_A = \begin{bmatrix} -\frac{1}{T_1} & 0 & \frac{A_3}{A_1 T_3} & 0 \\ 0 & -\frac{1}{T_2} & 0 & \frac{A_4}{A_2 T_4} \\ 0 & 0 & -\frac{1}{T_3} & 0 \\ 0 & 0 & 0 & -\frac{1}{T_4} \end{bmatrix}, \quad (50)$$

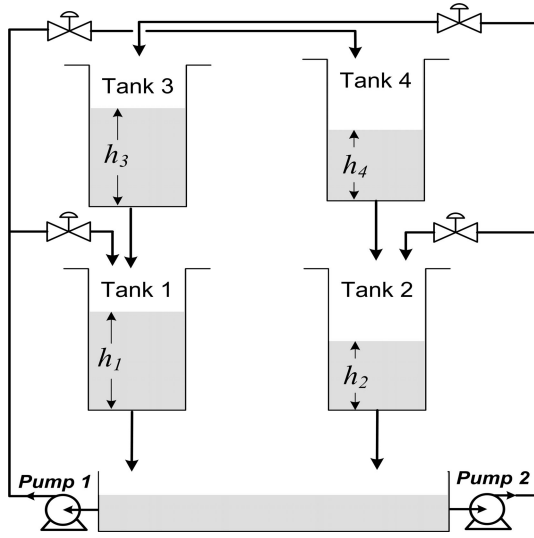


Fig. 2. Experimental four tank system scheme.

$$J_B = \begin{bmatrix} \frac{\gamma_1 k_1}{A_1} & 0 \\ 0 & \frac{\gamma_2 k_2}{A_3} \\ 0 & \frac{(1-\gamma_2)k_2}{A_3} \\ \frac{(1-\gamma_1)k_1}{A_4} & 0 \end{bmatrix}, \quad (51)$$

where

$$T_i = \frac{A_i}{a_i} \sqrt{\frac{2h_i(0)}{g}}.$$

The second step is to find $\hat{\Phi}$. Defining the state vector

$$\mathbf{x}(t) = [h_1(t) \ h_2(t) \ h_3(t) \ h_4(t)]^T$$

and a sample time $T = 0.5$ s, we have

$$\mathbf{x}(k+1) = \hat{\Phi} \mathbf{x}(k) + \hat{\Gamma} \mathbf{u}(k) + \mathbf{n}(k), \quad (52)$$

$$\hat{\Phi} = \begin{bmatrix} 0.991 & 0 & 0.013 & 0 \\ 0 & 0.990 & 0 & 0.016 \\ 0 & 0 & 0.987 & 0 \\ 0 & 0 & 0 & 0.984 \end{bmatrix}, \quad (53)$$

$$\hat{\Gamma} = \begin{bmatrix} 0.001 & 0 \\ 0 & 0.001 \\ 0 & 0.003 \\ 0.0025 & 0 \end{bmatrix}, \quad (54)$$

$$\mathbf{n}(k) = \begin{bmatrix} 0 & 0 \\ 0 & 0 \\ 0.2 & 0 \\ 0 & 0.3 \end{bmatrix} \mathbf{d}(k). \quad (55)$$

Since $\mathbf{x}_r = \mathbf{x}_e \neq 0$, the system dynamics must be specified in relation to the error vector $\mathbf{e}(k)$ defined as follows:

$$\mathbf{e}(k) = \mathbf{x}_r - \mathbf{x}(k), \quad \mathbf{x}_r = \mathbf{x}_e. \quad (56)$$

First we need to select a state vector feedback gain matrix \mathbf{K} such that the system given in (52) is asymptotically stable. Choosing an optimal procedure (MATLAB function `d1qr`), the following gain matrix \mathbf{K} is obtained:

$$\mathbf{K} = \begin{bmatrix} 30.967 & 39.236 & -14.700 & 82.493 \\ 37.259 & 23.677 & 85.482 & -15.328 \end{bmatrix}, \quad (57)$$

where \mathbf{P} and \mathbf{Q} are arbitrarily chosen as \mathbf{I}_n and $10^{-5}\mathbf{I}_n$, respectively. Then, the matrix \mathbf{E} must be specified.

Choosing the following arbitrary matrix \mathbf{E} :

$$\mathbf{E} = \mathbf{E}_1 = \begin{bmatrix} 1 & 0.01 \\ 0 & 1 \end{bmatrix}, \quad (58)$$

the switching surface is computed by means of the proposed switching surface equation given in (16):

$$\mathbf{C} = \begin{bmatrix} 31.6310 & 39.8851 & -14.4379 & 83.0338 \\ 37.6053 & 23.9244 & 86.1099 & -15.9645 \end{bmatrix}. \quad (59)$$

Using (22) for calculating the system matrix $\hat{\Phi}_e$ for the ideal SM, we have

$$\hat{\Phi}_e = \begin{bmatrix} 0.8364 & -0.1970 & 0.0926 & -0.4184 \\ -0.1686 & 0.8837 & -0.3921 & 0.0911 \\ -0.3746 & -0.2317 & 0.1001 & 0.1848 \\ -0.3028 & -0.3897 & 0.1705 & 0.1477 \end{bmatrix}, \quad (60)$$

and the ideal SM spectrum is

$$\Lambda(\hat{\Phi}_{SM}) = \{0.9889, 0.9791, 0, 0\}.$$

Therefore, the ideal SM is asymptotically stable. In order to illustrate the closed-loop stability, numerical simulations are performed as explained next.

Simulation. The numerical values are obtained using the computing environment MATLAB[®], and the controller was implemented using a control law obtained via the reaching law approach proposed by Gao *et al.* (1995) such that

$$\mathbf{u}(k) = \mathbf{u}_{equ}(k) - \mathbf{E}^{-1} [\mathbf{s}(k) (\mu T - 1) + \varepsilon T \text{sign}(\mathbf{s}(k))], \quad (61)$$

where the arbitrary designing parameters ε and μ must satisfy the following restriction:

$$\Delta = \frac{\varepsilon T}{1 - \mu T}, \quad (62)$$

where 2Δ corresponds to the width of the *quasi sliding mode band* (QSMB). For a QSMB < 1 and $\mu = 1$, ε becomes 0.5.

Tracking problem simulation. To illustrate how the system follows the reference value or set-point $\mathbf{x}_r(k)$,

let us consider a scenario where $\mathbf{x}_r(k)$ changes from $\mathbf{x}_r = \mathbf{x}_e$ to $\mathbf{x}_r = \mathbf{x}_e(1 + 20\%)$. Thus, the error vector value quickly raises up as shown in Fig. 3. Nevertheless, DVSC can drive the error vector to zero, which proves the asymptotically stability of the switching surface (see Figs. 5 and 4). Hence, the state vector signal values are driven from $\mathbf{x}(0)$ to the new reference, i.e., $\mathbf{x}(k)$ follows $\mathbf{x}_r(k)$ (see Fig. 5), and the surface values $\mathbf{s}(k)$, which are shown in Fig. 4, decay in a short time.

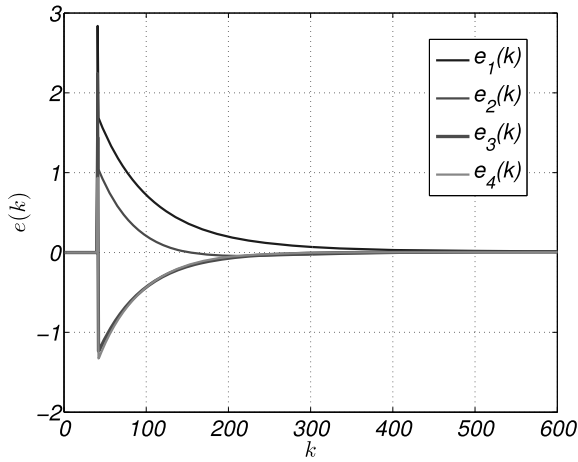


Fig. 3. Tracking error $\mathbf{e}(k)$.

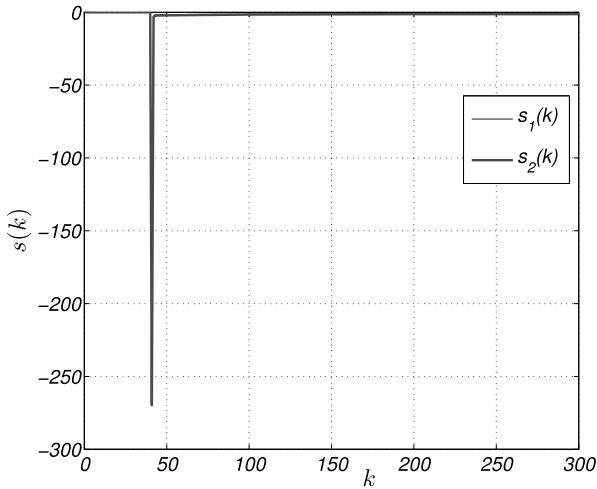


Fig. 4. Evolution of the sliding surface $\mathbf{s}(k)$.

Robustness analysis. In order to illustrate the robustness of the SM dynamics for a switching surface designed using the proposed methodology, two scenarios are presented. The first one considers an external disturbance which increases the level of Tank 3 by 0.5 cm for 5 s. In Fig. 6, it can be seen that the state vector value is perturbed

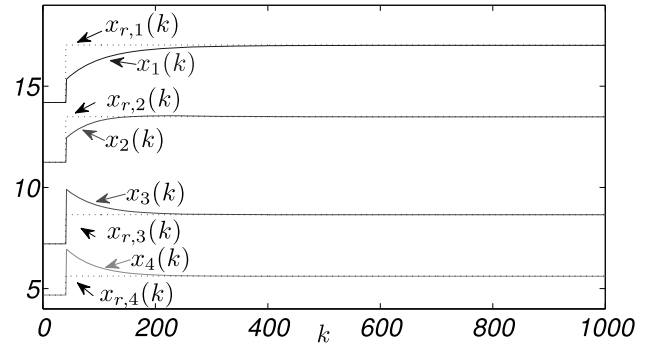


Fig. 5. Evolution of the state vector $\mathbf{x}(k)$ after a change in the reference value $\mathbf{x}_r(k)$.

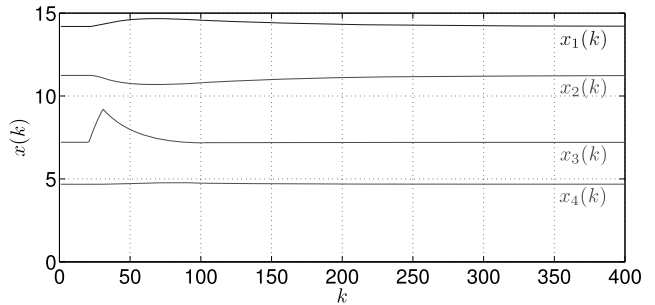


Fig. 6. Stable closed-loop system dynamics perturbed by the external disturbance $d_1(k)$.

at $t = 10$ s but recovers its stable stationary state \mathbf{x}_e about 200 s later. The switching surface $\mathbf{s}(k)$, the vector error $\mathbf{e}(k)$ and the control law $\mathbf{u}(k)$ dynamics are shown in Figs. 7–9, respectively.

The second robustness test consists in adding Gaussian noise $\eta(k)$ to the input $u_1(k)$, where the mean and variance of $\eta(k)$ are $E(\eta(k)) = 10$ and $\sigma(\eta(k)) = 10$, respectively (see Fig. 10). Despite this perturbation, the controller stabilizes the system around the stationary point $\mathbf{x}(0)$, as can be seen in Fig. 11.

Nonideal sliding mode considerations. To explain how the design parameter \mathbf{E} affects the nonideal sliding mode, let us chose another value for \mathbf{E} such that

$$\mathbf{E} = \mathbf{E}_2 = \begin{bmatrix} 4 & -3 \\ -3 & 4 \end{bmatrix}. \quad (63)$$

For the state vector feedback gain matrix \mathbf{K} given in (57), the following switching function is obtained with (16):

$$\mathbf{C}_2 = \begin{bmatrix} 12.204 & 86.811 & -319.526 & 380.667 \\ 56.656 & -23.240 & 390.337 & -313.438 \end{bmatrix}. \quad (64)$$

As expected, the system matrix $\hat{\Phi}_{SM,2}$ for the ideal SM for $\mathbf{C} = \mathbf{C}_2$ coincides with the one given in (60). For the simulations, the control law given in (61) is chosen, where

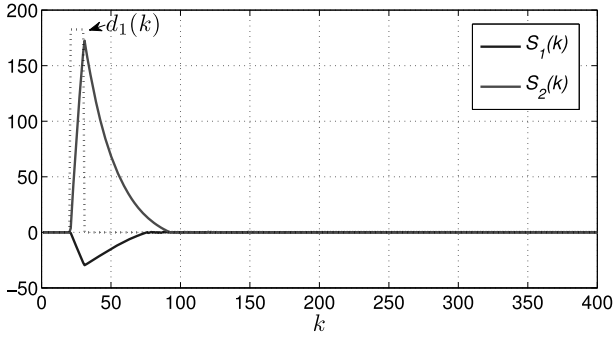


Fig. 7. Surface dynamics for the closed loop system simulated with the external disturbance $d_1(k)$.

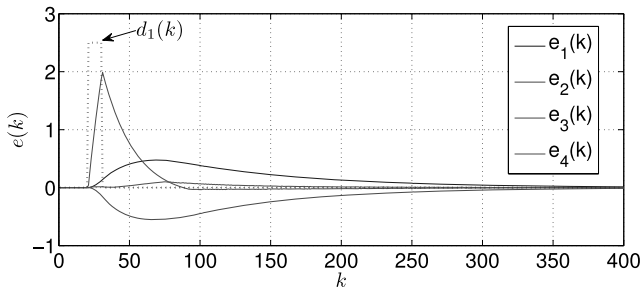


Fig. 8. Error dynamics $e(k)$ for the pulse disturbance $d_1(k)$.

$\mathbf{u}(k)$ is disturbed by the signal noise $\eta(k)$ previously defined. The control law is designed to guarantee that $\mathbf{s}(k) = 0$, i.e., $\mathbf{e}(k) = 0$ and, as can be seen in Fig. 12, it is achieved for both specifications matrix of \mathbf{E} . However, since $\mathbf{E}_1 \neq \mathbf{E}_2$, the control law effort differs considerably in each case, as can be seen in Fig. 13. Hence, it is clear that \mathbf{E} can be used for improving the controlled system performance during the sliding mode phase.

This numerical simulation shows that a switching surface specified as in (16) yields asymptotically stable nonideal sliding mode dynamics for nonlinear discrete time MIMO systems whose dynamics are given in the affine variable state representation. In addition, it is illustrated how the definition of the parameter \mathbf{E} affects the nonideal controlled system behaviour.

5. Conclusion and future works

This research work proposed a simple scheme for designing switching surfaces applied to a discrete time affine nonlinear MIMO system. The presented methodology makes use of linearized systems dynamics. We integrated the linearizing procedure with the surface scheme in a unique equation which leads to a novel and powerful design approach. Due to using the well-known control methodologies applied to linear systems, such as pole placement or LQR, the researcher can apply all of

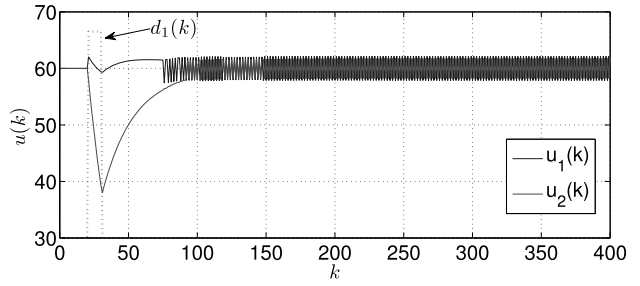


Fig. 9. Control law $\mathbf{u}(k)$ for perturbed closed loop systems.

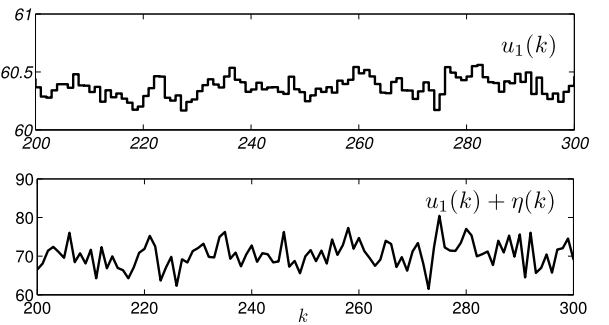


Fig. 10. Nominal control law $u_1(k)$ and the perturbed control law $\eta(k) + u_1(k)$.

these different design criteria to a nonlinear DVSC control problem.

The absence of any coordinate transformation eliminates the hard task of obtaining those, which in turn reduces the design effort. In addition, the proposed method is the only one that allows designers to adjust both the reaching and nonideal sliding modes through the matrix \mathbf{E} for nonlinear MIMO systems. Moreover, future research works that analyze the pseudo-sliding dynamics for a controlled system with the proposed switching surface scheme can be conducted in order to obtain new reaching law conditions or improved control laws. For all these reasons, this research work can be considered a useful tool for the design of sliding surfaces for controlling nonlinear MIMO systems via DVSC. The design rules presented for the design of DVSC according to the proposed methodology constitute an easy brief guideline for designers.

On the other hand, the proposed methodology makes use of the Jacobian or Taylor linearizing criteria. Since other optimal linearization approaches applied to nonlinear dynamical systems have been proposed (see Ababneh et al., 2011), these linearization methods can be used instead of the Jacobian criterion to verify if some performance features of the controlled system dynamics are improved.

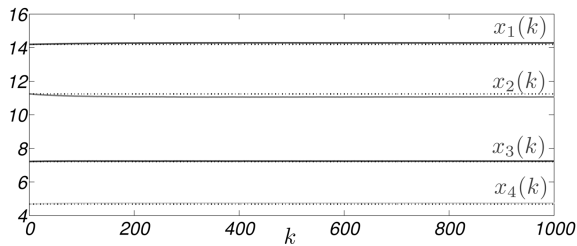


Fig. 11. State vector dynamics $x(k)$ for the disturbance $d_1(k)$.

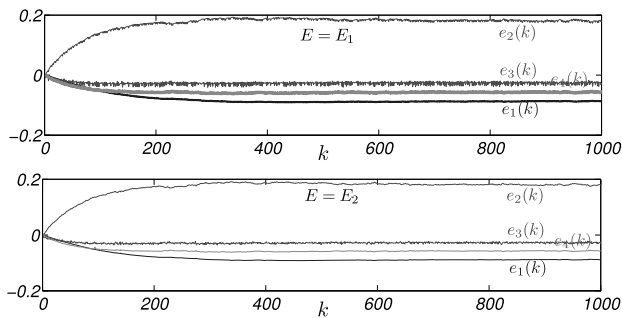


Fig. 12. Comparisons between the tracking error for $\mathbf{E} = \mathbf{E}_1$ and $\mathbf{E} = \mathbf{E}_2$.

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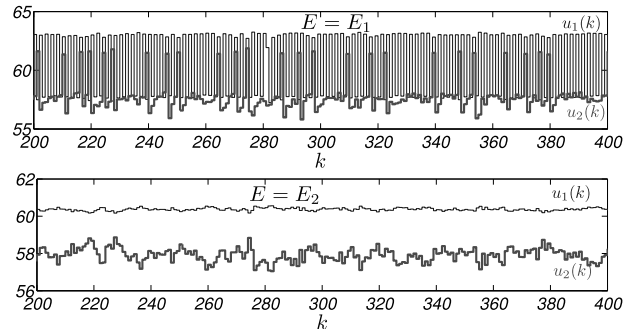


Fig. 13. Comparisons between the control law for $\mathbf{E} = \mathbf{E}_1$ and $\mathbf{E} = \mathbf{E}_2$.

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Appendix

A1. First order Taylor expansion term linearization method

Given $f : \mathbb{R} \rightarrow \mathbb{R}$ such that $f(x)$ is infinitely many times differentiable at some complex or real point x_e , $f(\cdot)$ can be approximated around x_e through the following Taylor expansion:

$$f(x) = \sum_{i=0}^{\infty} \frac{f^{(i)}(x_e)}{i!} (x - x_e)^i, \quad (\text{A1})$$

where $f^{(i)}$ denotes the i -th derivative of f . For the first term of (A1), we have

$$f(x) \approx f(x_e) + f'(x_e)(x - x_e). \quad (\text{A2})$$

For a general dynamic system

$$\dot{x}(t) = f(x), \quad (\text{A3})$$

assume that for $x = x_e$ we have $f(x_e) = 0$. For the case of $x_e = 0$, we have

$$\dot{x}(t) \approx f'(0)(x(t) - x_e). \quad (\text{A4})$$

For the general multivariable case $\mathbf{f} : \mathbb{R}^n \rightarrow \mathbb{R}^n$, i.e., for $\mathbf{f}(\cdot)$ defined as

$$\mathbf{f}(x) = \begin{bmatrix} f_1(x) \\ f_2(x) \\ \vdots \\ f_n(x) \end{bmatrix}, \quad (\text{A5})$$

where $x(t) = [x_1(t) \ x_2(t) \ \dots \ x_n(t)]$, we have

$$\dot{x}(t) \approx D\mathbf{f}(x_e)(x(t) - x_e) \quad (\text{A6})$$

where $D\mathbf{f}(x_e)$ is the Jacobian matrix defined as

$$D\mathbf{f}(x) = \mathbf{J} = \begin{bmatrix} \frac{\partial f_1}{\partial x_1} & \frac{\partial f_1}{\partial x_2} & \dots & \frac{\partial f_1}{\partial x_n} \\ \frac{\partial f_2}{\partial x_1} & \frac{\partial f_2}{\partial x_2} & \dots & \frac{\partial f_2}{\partial x_n} \\ \vdots & \vdots & \ddots & \vdots \\ \frac{\partial f_n}{\partial x_1} & \frac{\partial f_n}{\partial x_2} & \dots & \frac{\partial f_n}{\partial x_n} \end{bmatrix}. \quad (\text{A7})$$

A2. Forward Euler method

The well-known forward Euler method, or simply the Euler method, is an explicit numerical approximation methodology for numerically solving ordinary differential equations, which produces first-order solutions. For the differential equation

$$\dot{x}(t) = f(x, t) \quad (\text{A8})$$

a numerical approximation of $x(t)$ at $t = k_0 + kT$, where $k \in \mathbb{Z}$ is an integer time step with temporal separation of T , can be made using

$$x(k+1) = x(k) + Tf(k, x(k)). \quad (\text{A9})$$

It is known that the global approximation error is proportional to the step size T , and therefore the global error decreases as $T \rightarrow 0$.

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